MPQ8633A-H

16V, 12A, Configurable-Frequency, Synchronous Step-Down Converter with Adjustable Current Limit and Voltage Tracking

DESCRIPTION

The MPQ8633A-H is a fully integrated, high-frequency, synchronous step-down converter. It offers a very compact solution that can achieve up to 12A of output current (I_{OUT}) across a wide input voltage (V_{IN}) range, with excellent load and line regulation. The MPQ8633A-H operates at high efficiency across a wide I_{OUT} load range.

Internally compensated constant-on-time (COT) control provides fast transient response and eases loop stabilization.

The selectable switching frequency (f_{SW}) can be set to 600kHz, 800kHz, or 1000kHz by configuring the MODE pin. This maintains a constant f_{SW}, regardless of V_{IN} and the output voltage (V_{OUT}).

During start-up, the internal soft-start timer (t_{SS}) (1ms) ramps up V_{OUT} in a controlled manner. t_{SS} can be increased by adding a capacitor on the TRK/REF pin. An open-drain power good (PG) signal indicates whether V_{OUT} is within its nominal voltage range. If the input fails to supply power to the MPQ8633A-H, then the PG voltage (V_{PG}) is clamped at about 0.7V via an external pull-up voltage.

Full protection features include over-current protection (OCP), over-voltage protection (OVP), under-voltage protection (UVP), and over-temperature protection (OTP).

The MPQ8633A-H requires a minimal number of readily available, standard external components, and is available in a QFN-21 (3mmx4mm) package.

FEATURES

- Wide Input Voltage (V_{IN}) Range:
  - 2.7V to 16V with External 3.3V Bias
  - 4V to 16V with Internal Bias or External 3.3V Bias
- Differential Output Voltage (V_{OUT}) Remote Sense
- Configurable Accurate Current Limit (I_{LIMIT})
- 12A Output Current (I_{OUT})
- Integrated Low $R_{DS(ON)}$ Power MOSFETs
- Proprietary Switching Loss Reduction Technique
- Adaptive Constant-On-Time (COT) Control for Ultrafast Transient Response
- Stable with Zero ESR Output Capacitor
- Reference Voltage (V_{REF}) Accuracy:
  - 0.5% V_{REF} Accuracy from 0°C to 70°C
  - 1% V_{REF} Accuracy from -40°C to +125°C
- Selectable Pulse-Skip Mode (PSM) or Forced Continuous Conduction Mode (FCCM)
- Excellent Load Regulation
- V_{OUT} Tracking
- V_{OUT} Discharge
- PGOOD Clamped Low during Power Failure
- Configurable Soft-Start Time (t_{SS}) from 1ms
- Pre-Biased Start-Up
- 600kHz, 800kHz, or 1000kHz Selectable Switching Frequency (f_{SW})
- Non-Latch OCP, UVP, OVP, UVLO Protection, and Thermal Shutdown
- Adjustable V_{OUT} from 0.6V to 90% of V_{IN} (5.5V Max)
- Available in a QFN-21 (3mmx4mm) Package

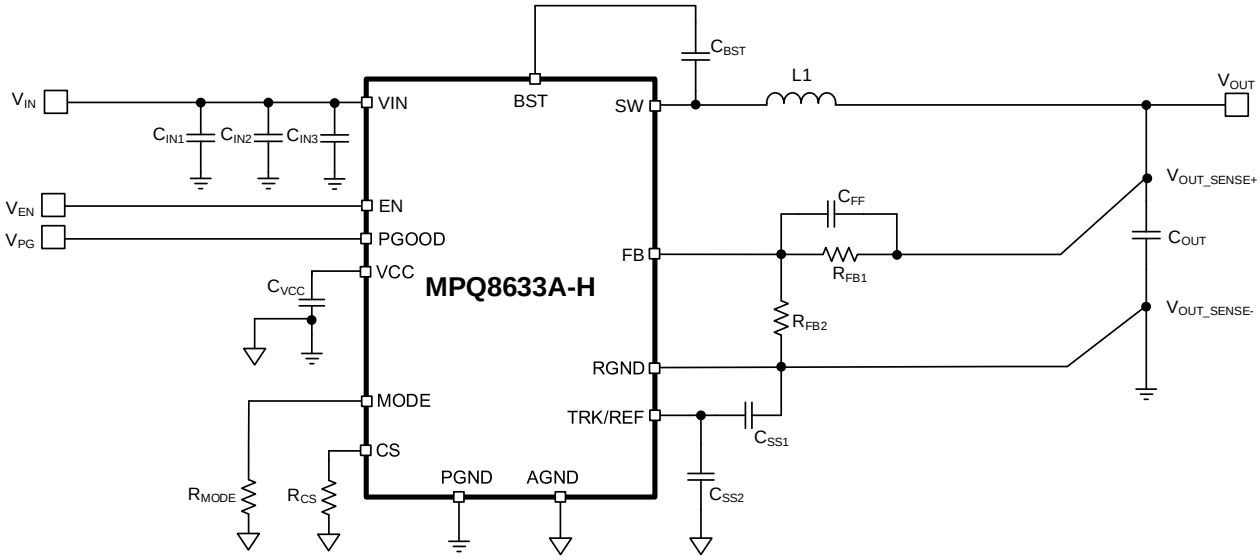
APPLICATIONS

- Telecommunication Systems
- Networking Systems
- Servers
- Base Stations

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TYPICAL APPLICATION



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ORDERING INFORMATION

Part Number*	Package	Top Marking	MSL Rating
MPQ8633A-HGLE	QFN-21 (3mmx4mm)	*See Below*	1

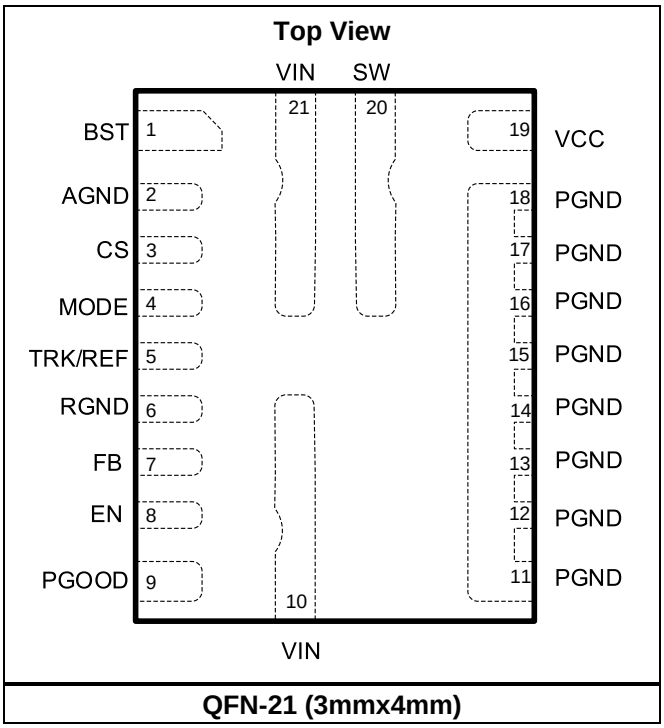
For Tape & Reel, add suffix -Z (e.g. MPQ8633A-HGLE-Z).

TOP MARKING

MPYW
8633
ALLL
EH

MP: MPS prefix
Y: Year code
W: Week code
8633A: First five digits of the part number
LLL: Lot number
E: Package prefix
H: Non-latch OVP

PACKAGE REFERENCE



QFN-21 (3mmx4mm)

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PIN FUNCTIONS

Pin #	Name	Description
1	BST	**Bootstrap**. Connect a capacitor between the SW and BST pins to form a floating supply across the high-side MOSFET (HS-FET) driver.
2	AGND	**Analog ground.** Select the AGND pin to be the control circuit reference point.
3	CS	**Current limit.** Connect a resistor between the CS pin and AGND to set the current limit (I_{LIMIT}) trip point.
4	MODE	**Mode selection**. Configure the MODE pin to select either forced continuous conduction mode (FCCM) or pulse-skip mode (PSM). MODE also selects the switching frequency (f_{SW}). See table 1 on page 14 for additional details.
5	TRK/REF	**External voltage-tracking input.** The output voltage (V_{OUT}) tracks the TRK/REF input signal. Use a ceramic decoupling capacitor to decouple the TRK/REF pin. Place this capacitor as close to TRK/REF as possible. Capacitors with X7R or X5R grade dielectrics are recommended due to their stable temperature characteristics. The TRK/REF capacitor ($C_{TRK/REF}$) determines the soft-start time (t_{SS}). See Equation 2 on page 14 for additional details.
6	RGND	**Differential remote-sense negative input.** Connect the RGND pin directly to the negative side of the voltage-sensing point. Short RGND to PGND if remote sense is not used.
7	FB	**Feedback and differential remote-sense positive input.** An external resistor divider connected between the output and RGND (tapped to the FB pin) sets V_{OUT}. Place this resistor divider as close to FB as possible. Do not use vias on the FB traces.
8	EN	**Enable**. The EN pin is an input signal that turns the converter on and off. Pull EN high to turn the converter on; pull EN low to turn it off. Connect the EN and VIN pins via a pull-up resistor or a resistive voltage divider for automatic start-up. Do not float EN.
9	PGOOD	**Power good output.** The PGOOD pin is an open-drain output. A pull-up resistor connected to a DC voltage is required to indicate whether V_{OUT} is within the regulation voltage range. If the output is in regulation, PGOOD is pulled high. There is a delay (about 1ms) between when the FB voltage (V_{FB}) exceeds 92.5% and the PGOOD voltage (V_{PG}) is pulled high.
10, 21	VIN	**Input voltage.** The VIN pin supplies power to the internal MOSFET and converter. Use decoupling input capacitors to decouple the input rail. Use wide PCB traces to make the VIN connection.
11, 12, 13, 14, 15, 16, 17, 18	PGND	**System ground.** The PGND pin is the reference ground of the regulated V_{OUT}, and requires careful consideration when designing the PCB layout. Use wide PCB traces to make the PGND connection.
19	VCC	**Internal 3V LDO output.** The driver and the control circuitry are powered by the VCC pin. Use a ≥1µF ceramic decoupling capacitor to decouple VCC. Place this capacitor as close to VCC as possible. Capacitors with X7R or X5R grade dielectrics recommended due to their stable temperature characteristics.
20	SW	**Switch output.** Connect the SW pin to the inductor and the bootstrap capacitor (C_{BST}). SW is pulled up to the VIN voltage (V_{IN}) by the HS-FET during the pulse-width modulation (PWM) duty cycle on time (t_{ON}). SW is pulled low by the inductor current (I_L) during the PWM off time (t_{OFF}). Use wide PCB traces to make the SW connection.

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ABSOLUTE MAXIMUM RATINGS (1)

Input voltage (V_{IN}) 18V
V_{SW} (DC) .....-0.3V to V_{IN} + 0.3V
V_{SW} (25ns) (2).....-3V to +25V
V_{SW} (25ns).....-5V to +25V
V_{BST} ..... V_{SW} + 4V
V_{CC}, V_{EN}..... 4.5V
All other pins .....-0.3V to +4.3V
Junction temperature .....170°C
Lead temperature .....260°C
Storage temperature ..... -65°C to +170°C

Recommended Operating Conditions (3)

Input voltage (V_{IN}) .....4V to 16V
V_{IN} (DC) - V_{SW} (DC) (4).....-0.3V to V_{IN} + 0.3V
V_{SW} (DC) (4) .....-0.3V to V_{IN} + 0.3V
Output voltage (V_{OUT}).....0.6V to 5.5V
External VCC Bias (V_{CC_EXT}) .....3.12V to 3.6V
Max output current (I_{OUT_MAX}) 12A
Max output current limit (I_{LIMIT_MAX}) 16A
Max peak inductor current ($I_{L_PEAK_MAX}$) 18A
EN voltage (V_{EN}) 3.6V
Operating junction temp (T_J).... -40°C to +125°C

Thermal Resistance (5) (6) θ_{JB} θ_{JC_TOP}

QFN-21 (4mmx3mm) ……9……21.....°C/W

Notes:

1) Exceeding these ratings may damage the device.
2) Measured using a differential oscilloscope probe.
3) The device is not guaranteed to function outside of its operating conditions.
4) If V_{IN} is 16V, then the voltage rating can be between -3V and +23V for ≤25ns, with a maximum repetition rate of 1000kHz.
5) θ_{JB} is the thermal resistance from the junction to the board around the PGND pin's soldering point.
6) θ_{JC_TOP} is the thermal resistance from the junction to the top of the package.

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ELECTRICAL CHARACTERISTICS

V_{IN} = 12V, T_J = -40°C to +125°C, unless otherwise noted.

Parameters	Symbol	Condition	Min	Typ	Max	Units
Supply Currents						
Shutdown current	I_{SD}	V_{EN} = 0V		10	20	µA
Quiescent current	I_Q	V_{EN} = 2V, V_{FB} = 0.62V		650	850	µA
MOSFETs						
High-side MOSFET (HS-FET) switch leakage	$I_{SW_LKG_HS}$	V_{EN} = 0V, V_{SW} = 0V		0	10	µA
Low-side MOSFET (LS-FET) switch leakage	$I_{SW_LKG_LS}$	V_{EN} = 0V, V_{SW} = 12V		0	30	
HS-FET on resistance	$R_{DS(ON)_HS}$	V_{EN} = 2V, T_J = 25°C		13.3		mΩ
LS-FET on resistance	$R_{DS(ON)_LS}$	V_{EN} = 2V, T_J = 25°C		3.8		mΩ
Current Limit (I_{LIMIT})						
Current limit threshold	V_{LIMIT}		1.15	1.2	1.25	V
I_{CS} to I_{OUT} ratio	I_{CS} / I_{OUT}	I_{OUT} ≥ 2A	18	20	22	µA/A
LS-FET negative current limit	I_{LIMIT_NEG}			-9		A
Negative current limit timer (7)	t_{NCL}			200		ns
Switching Frequency (f_{SW})						
Switching frequency (8)	f_{SW}	R_{MODE} is pulled to AGND, I_{OUT} = 0A, V_{OUT} = 1V	480	600	720	kHz
		R_{MODE} = 30.1kΩ, I_{OUT} = 0A, V_{OUT} = 1V	680	800	920	kHz
		R_{MODE} = 60.4kΩ, I_{OUT} = 0A, V_{OUT} = 1V	850	1000	1150	kHz
Minimum on time (7)	t_{ON_MIN}	V_{FB} = 500mV			50	ns
Minimum off time (7)	t_{OFF_MIN}	V_{FB} = 500mV			180	ns
Over-Voltage Protection (OVP) and Under-Voltage Protection (UVP)						
OVP threshold	V_{OVP}		113	116	119	% of V_{REF}
UVP threshold	V_{UVP}		77	80	83	% of V_{REF}
Feedback (FB) and Soft Start (SS)						
Reference voltage	V_{REF}	T_J = -40°C to +125°C	594	600	606	mV
		T_J = 0°C to +70°C	597	600	603	mV
TRK/REF source current	$I_{SOURCE_TRK/REF}$	$V_{TRK/REF}$ = 0V		42		µA
TRK/REF sink current	$I_{SINK_TRK/REF}$	$V_{TRK/REF}$ = 1V		12		µA
Soft-start time	t_{SS}	$C_{TRK/REF}$ = 1nF, T_J = 25°C	0.75	1	1.25	ms
Error Amplifier (EA)						
EA offset	V_{OFFSET}		-3	0	+3	mV
FB current	I_{FB}	V_{FB} = V_{REF}		50	100	nA

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ELECTRICAL CHARACTERISTICS *(continued)*

V_{IN} = 12V, T_J = -40°C to +125°C, unless otherwise noted.

Parameters	Symbol	Condition	Min	Typ	Max	Units
Enable (EN) and Under-Voltage Lockout (UVLO) Protection						
EN rising threshold	V_{EN_RISING}		1.17	1.22	1.27	V
EN hysteresis	V_{EN_HYS}			200		mV
EN current	I_{EN}	V_{EN} = 2V		0		µA
Soft-shutdown discharge MOSFET on resistance	$R_{DS(ON)_DISCHARGE}$			80	150	Ω
V_{IN} UVLO						
V_{IN} UVLO rising threshold	$V_{IN_UVLO_RISING}$	V_{CC} = 3.3V	2.1	2.4	2.7	V
V_{IN} UVLO falling threshold	$V_{IN_UVLO_FALLING}$	V_{CC} = 3.3V	1.55	1.85	2.15	V
VCC Regulator						
VCC UVLO rising threshold	$V_{CC_UVLO_RISING}$		2.65	2.8	2.95	V
VCC UVLO falling threshold	$V_{CC_UVLO_FALLING}$		2.35	2.5	2.65	V
VCC voltage	V_{CC}		2.88	3.00	3.12	V
VCC load regulation		I_{CC} = 25mA		0.5		% of V_{CC}
Power Good (PG)						
PG rising high threshold	$V_{PG_RISING_HIGH}$	V_{FB} is pulled high	89.5	92.5	95.5	% of V_{REF}
PG rising low threshold	$V_{PG_RISING_LOW}$	V_{FB} is pulled high	113	116	119	% of V_{REF}
PG falling high threshold	$V_{PG_FALLING_HIGH}$	V_{FB} is pulled low	98	101	104	% of V_{REF}
PG falling low threshold	$V_{PG_FALLING_LOW}$	V_{FB} is pulled low	77	80	83	% of V_{REF}
PG low to high delay	t_{PG}	T_J = 25°C	0.6	0.9	1.2	ms
PG sink current capability	V_{PG_SINK}	I_{PG} = 10mA			0.4	V
PG leakage current	I_{PG_LKG}	V_{PG} = 3.3V			3	µA
PG output voltage low level	$V_{OUT_LOW_100}$	V_{IN} = 0V, V_{PG} is pulled up to 3.3V via a 100kΩ resistor, T_J = 25°C		650	800	mV
	$V_{OUT_LOW_10}$	V_{IN} = 0V, V_{PG} is pulled up to 3.3V via a 10kΩ resistor, T_J = 25°C		750	900	mV
Thermal Shutdown						
Thermal shutdown (7)	T_{SD}			160		°C
Thermal shutdown hysteresis (7)				30		°C

Notes:

7) Guaranteed by design.
8) Guaranteed by design to remain in the specified range across different temperature ranges.

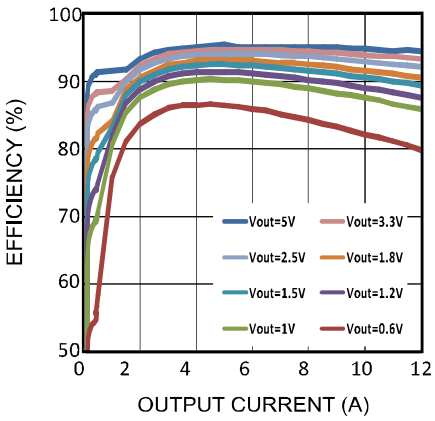
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TYPICAL PERFORMANCE CHARACTERISTICS

V_{IN} = 12V, T_A = 25°C, V_{OUT} = 1.2V, f_{SW} = 800kHz, unless otherwise noted.

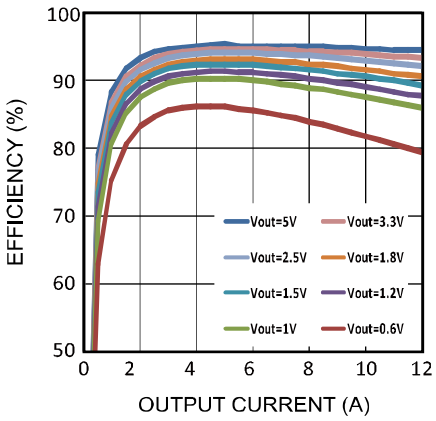
Efficiency

PSM, L = 1.1µH, f_{SW} = 800kHz



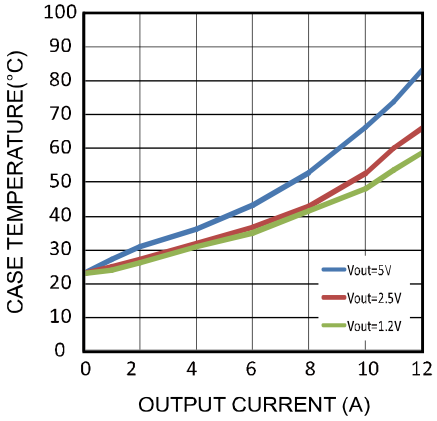
Efficiency

FCCM, L = 1.1µH, f_{SW} = 800kHz



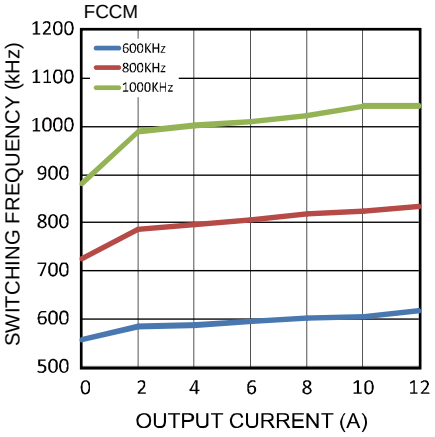
CaseTemperature Rise

f_{SW} = 800kHz

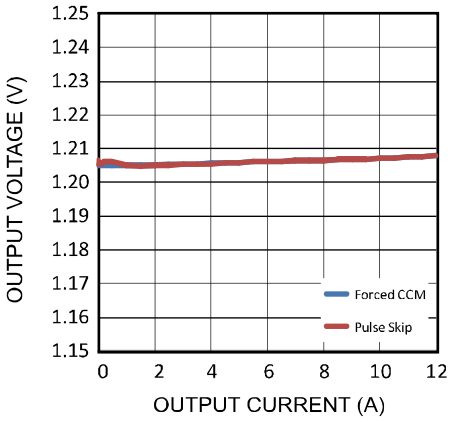


Switching Frequency vs. Output Current

FCCM



Load Regulation

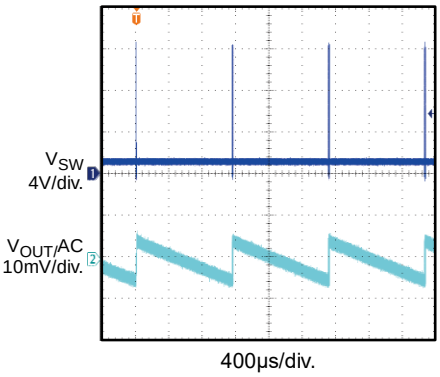


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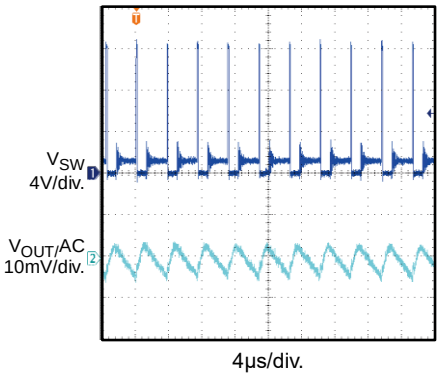
TYPICAL PERFORMANCE CHARACTERISTICS *(continued)*

Performance waveforms are tested on the evaluation board.

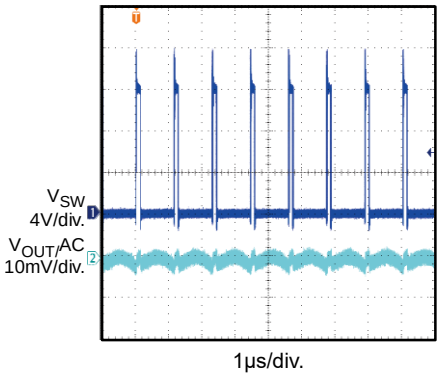
Steady State
I_{OUT} = 0A, PSM



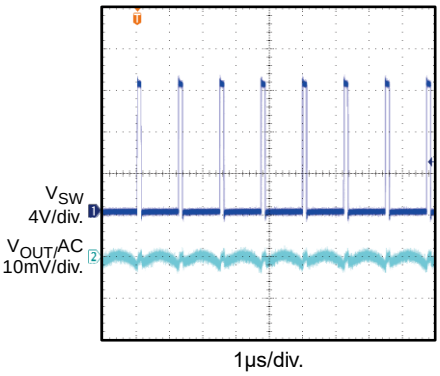
Steady State
I_{OUT} = 0.5A, PSM



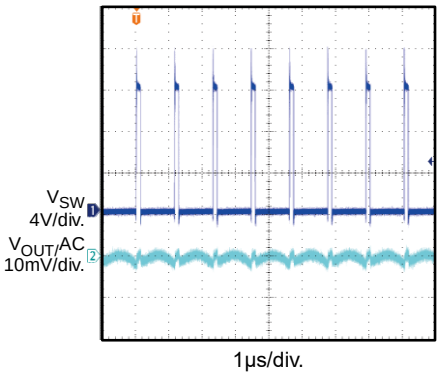
Steady State
I_{OUT} = 12A, PSM



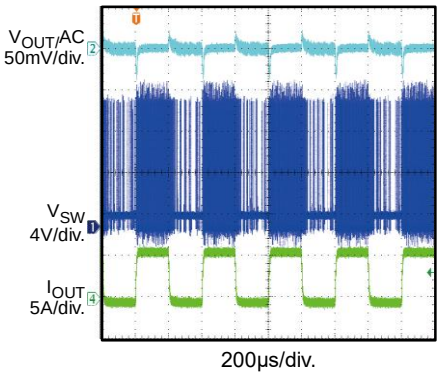
Steady State
I_{OUT} = 0A, FCCM



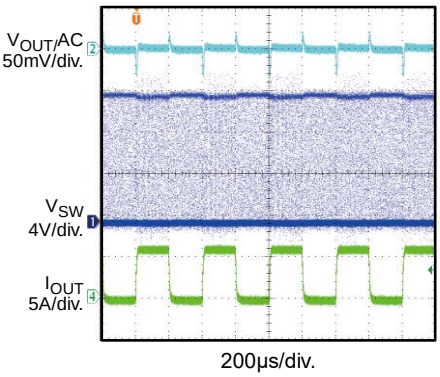
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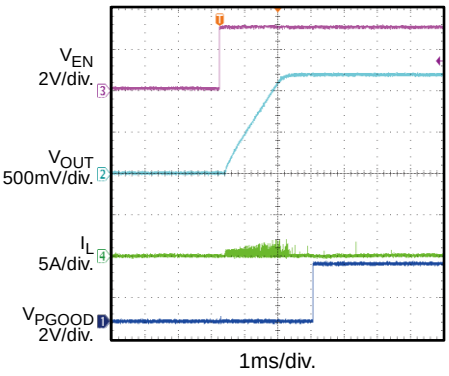
Load Transient
I_{OUT} = 0A to 6A, PSM



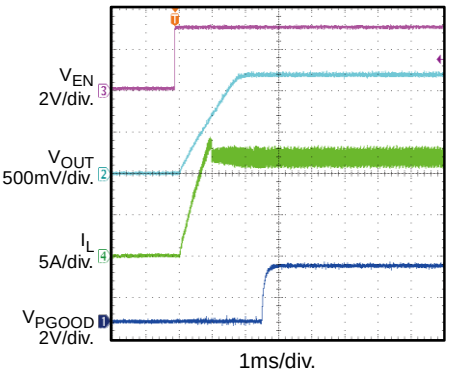
Load Transient
I_{OUT} = 0A to 6A, FCCM



Start-Up through EN
I_{OUT} = 0A, PSM



Start-Up through EN
I_{OUT} = 12A, PSM

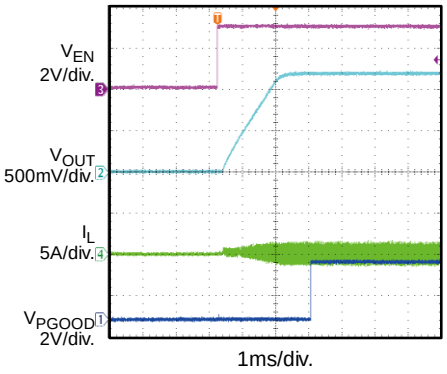


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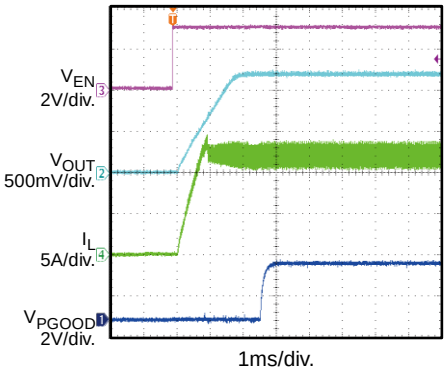
TYPICAL PERFORMANCE CHARACTERISTICS *(continued)*

Performance waveforms are tested on the evaluation board.

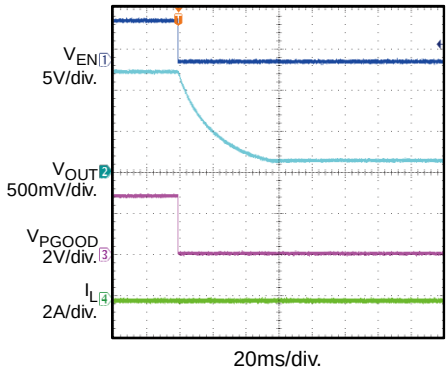
Start-Up through EN
I_{OUT} = 0A, FCCM



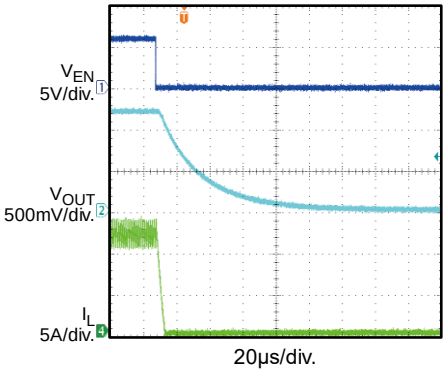
Start-Up through EN
I_{OUT} = 12A, FCCM



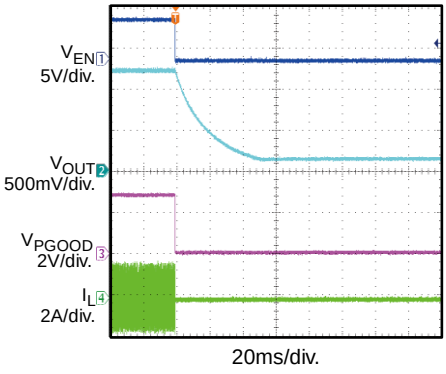
Shutdown through EN
I_{OUT} = 0A, PSM



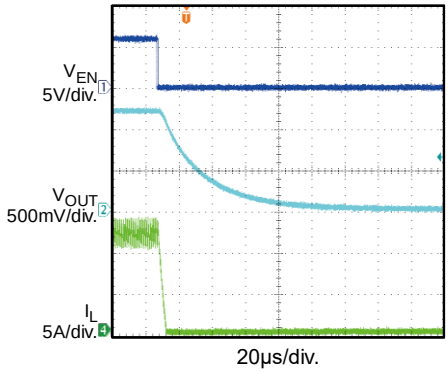
Shutdown through EN
I_{OUT} = 12A, PSM



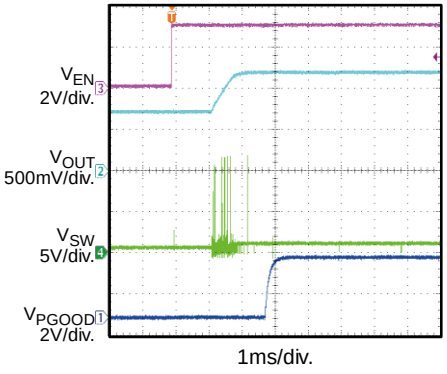
Shutdown through EN
I_{OUT} = 0A, FCCM



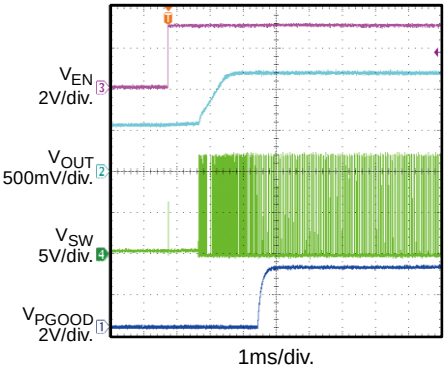
Shutdown through EN
I_{OUT} = 12A, FCCM



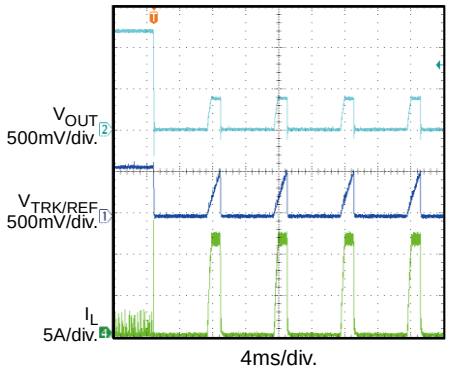
Pre-Bias Start-Up
PSM



Pre-Bias Start-Up
FCCM



OCP Entry

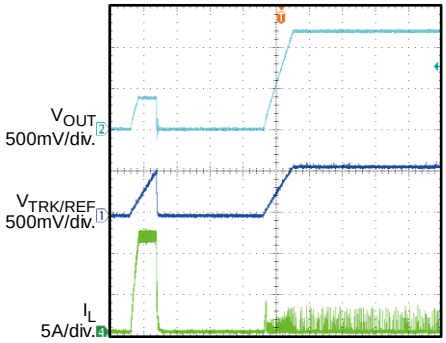


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TYPICAL PERFORMANCE CHARACTERISTICS *(continued)*

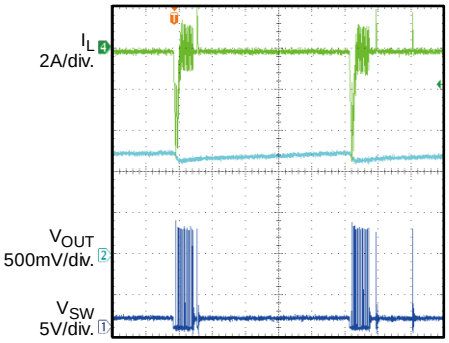
Performance waveforms are tested on the evaluation board.

OCP Recovery



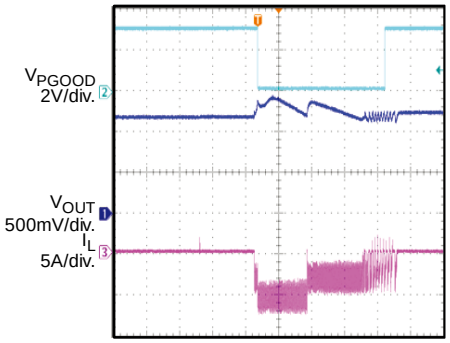
Output Sink Mode

PSM



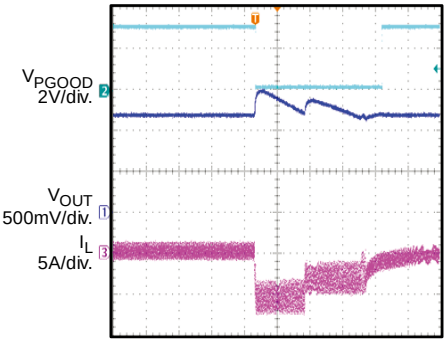
Over-Voltage Protection

PSM



Over-Voltage Protection

FCCM



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FUNCTIONAL BLOCK DIAGRAM

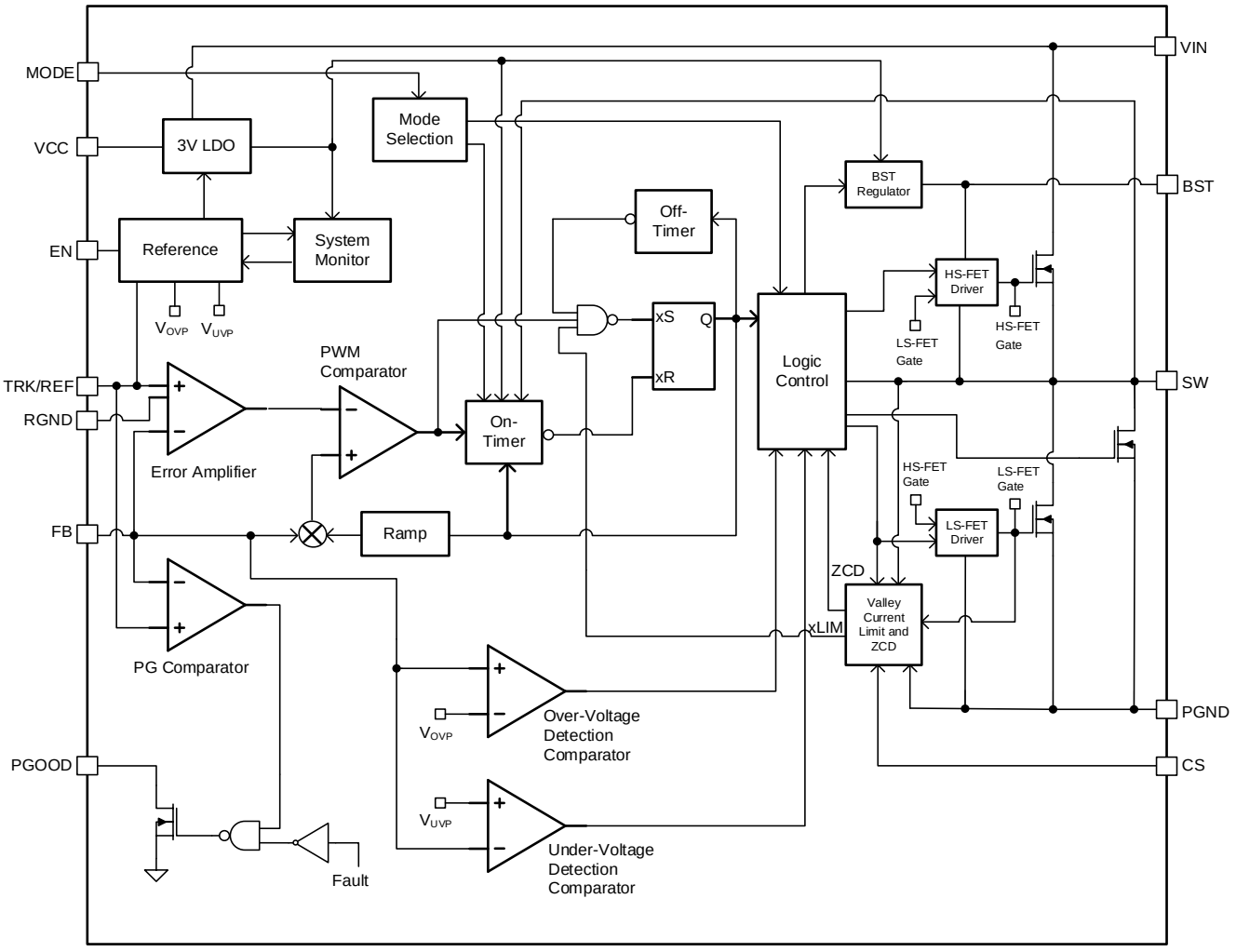


Figure 1: Functional Block Diagram

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OPERATION

Constant-On-Time (COT) Control

Constant-on-time (COT) control provides fast load transient response and eases loop stabilization. Figure 2 shows COT control.

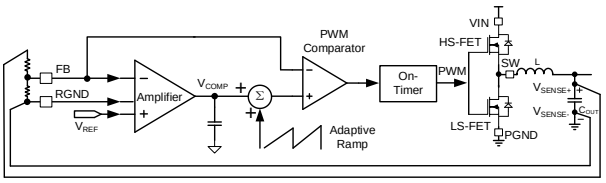


Figure 2: COT Control

The operational amplifier corrects any error voltage between the FB voltage (V_{FB}) and the reference voltage (V_{REF}). With the amplifier, the MPQ8633A-H can provide excellent load regulation across the entire load range, regardless of the operation mode.

The dedicated RGND pin provides differential output voltage (V_{OUT}) remote sensing. The remote-sensing traces should be kept in a low-impedance state for the best performance.

The MPQ8633A-H includes internal ramp compensation to support the low ESR MLCC output capacitor (C_{OUT}) solution. Adaptive internal ramp compensation provides stability across the entire input voltage (V_{IN}) range and V_{OUT} range with proper design of the output L/C filter.

Pulse-Width Modulation (PWM)

The amplifier corrects any error voltage between V_{FB} and V_{REF}, and generates a fairly smooth DC comparator (COMP) voltage (V_{COMP}). The internal ramp is superimposed onto COMP. The superimposed V_{COMP} is compared to V_{FB}. If V_{FB} drops below V_{COMP}, then the integrated high-side MOSFET (HS-FET) turns on. The HS-FET remains on for a fixed on time (t_{ON}). This fixed t_{ON} is determined by V_{IN}, V_{OUT}, and the selected switching frequency (f_{SW}). Once t_{ON} finishes, the HS-FET turns off. The HS-FET turns on again once V_{FB} drops below V_{COMP}. By repeating this operation, the MPQ8633A-H regulates V_{OUT}. The integrated low-side MOSFET (LS-FET) turns on once the HS-FET turns off to minimize conduction loss. If both the HS-FET and the LS-FET turn on simultaneously, then a dead short occurs between the VIN and PGND pins. This is known as shoot-through. To avoid shoot-through, a dead time (DT) is inserted between the HS-FET off time (t_{OFF}) and the LS-FET t_{ON}, and vice versa.

Figure 3 shows PWM mode under heavy-load conditions.

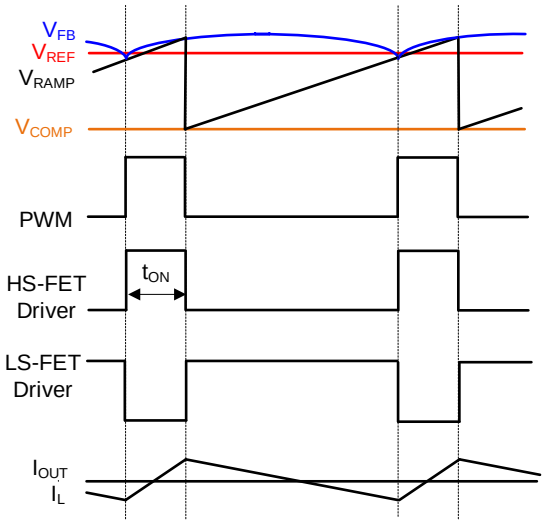


Figure 3: PWM Mode at Heavy-Loads

Forced Continuous Conduction Mode (FCCM)

If the output current (I_{OUT}) is high, and the inductor current (I_L) exceeds 0A, then the part operates in forced continuous conduction mode (FCCM) (see Figure 3). The MPQ8633A-H can also be configured to operate in FCCM while I_{OUT} is low (see the Mode Selection section on page 14).

In FCCM, f_{SW} is fairly constant (PWM mode), and the V_{OUT} ripple (ΔV_{OUT}) remains fairly constant across the entire load range.

Pulse-Skip Mode (PSM)

Under light-load conditions, the MPQ8633A-H can be configured to operate in pulse-skip mode (PSM) to optimize efficiency (see the Mode Selection section on page 14). I_L decreases as the load decreases. Once I_L reaches 0A, the part transitions from FCCM to PSM.

Figure 4 on page 14 shows PSM under light-load conditions.

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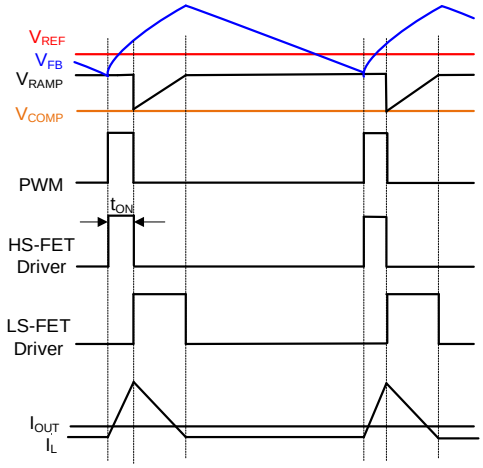


Figure 4: PSM at Light Loads

If V_{FB} drops below V_{COMP}, then the HS-FET turns on for a fixed interval. Once the HS-FET turns off, the LS-FET turns on until I_L reaches 0A. In PSM, V_{FB} should not reach V_{COMP} as I_L reaches 0A. The LS-FET driver enters a high-impedance (Hi-Z) state as I_L reaches 0A. A current modulator takes control of the LS-FET and limits I_L below -1mA, and the output capacitors discharge to PGND slowly via the LS-FET. In PSM, the HS-FET does not turn on as frequently as it does in FCCM. As a result, the efficiency in PSM is higher than that in FCCM.

As I_{OUT} increases, the current modulator regulation time decreases. The HS-FET turns on more frequently, and f_{SW} increases accordingly. I_{OUT} reaches its critical level once the current modulator time is 0s. The critical level of I_{OUT} can be calculated with Equation (1):

$$I_{OUT} = \frac{(V_{IN} - V_{OUT}) \times V_{OUT}}{2 \times L \times f_{SW} \times V_{IN}} \quad (1)$$

The part enters PWM mode once I_{OUT} exceeds its critical level. Then f_{SW} remains fairly constant across the entire I_{OUT} range.

The MPQ8633A-H can be configured to operate in FCCM while under light-load conditions (see Table 1).

Mode Selection

The MPQ8633A-H provides both FCCM and PSM for light-load operation. It also has three selectable f_{SW} options. The MODE resistor (R_{MODE}) selects f_{SW} and the operation mode under light-load conditions (see Table 1).

Table 1: Mode Selection at Light-Loads

R_{MODE}	Mode	f_{SW} (kHz)
Pulled to VCC	PSM	600
243kΩ (±20%) or pulled to AGND	PSM	800
121kΩ (±20%) or pulled to AGND	PSM	1000
Pulled to AGND	FCCM	600
30.1kΩ (±20%) or pulled to AGND	FCCM	800
60.4kΩ (±20%) or pulled to AGND	FCCM	1000

Soft Start (SS)

The minimum soft-start time (t_{SS}) is limited at 1ms. t_{SS} can be increased by adding a soft-start capacitor (C_{SS}) between the TRK/REF and RGND pins.

C_{SS} can be calculated with Equation (2):

$$C_{SS}(nF) = \frac{t_{SS}(ms) \times 36\mu A}{0.6(V)} \quad (2)$$

Output Voltage Tracking and Reference

TRK/REF is an analog input pin that can track another power supply or accept an external reference. If an external voltage signal is connected to TRK/REF, then TRK/REF acts as a reference for V_{OUT}. V_{FB} follows this external voltage signal, and the soft-start settings are ignored. The TRK/REF input signal can be between 0.3V and 1.4V. During start-up, the TRK/REF voltage ($V_{TRK/REF}$) should exceed 600mV to ensure proper operation. After start-up, $V_{TRK/REF}$ can be between 0.3V and 1.4V.

Pre-Biased Start-Up

The MPQ8633A-H is designed for a monotonic start-up into a pre-biased load. If the output is pre-biased to a certain voltage during start-up, then the IC turns both the HS-FET and LS-FET off until $V_{TRK/REF}$ exceeds the sensed voltage on the FB pin. If the BST voltage (V_{BST}) drops below the 2.3V before $V_{TRK/REF}$ exceeds the sensed voltage on the FB pin, then the LS-FET turns on to charge V_{BST} via VCC. The LS-FET turns on for very short pulses, so that the drop in the pre-biased level is negligible.

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Output Voltage Discharge

If the MPQ8633A-H shuts down through EN, then V_{OUT} discharge mode is enabled. Both the HS-FET and the LS-FET latch off, and a discharge MOSFET connected between the SW and PGND pins turns on to discharge V_{OUT}. The typical on resistance of this MOSFET is 80Ω. Once V_{FB} drops below 10% of V_{REF}, the discharge MOSFET turns off.

Current Sense and Over-Current Protection (OCP)

The MPQ8633A-H features an on-die current sense and a configurable positive current limit (I_{LIMIT}) threshold.

I_{LIMIT} is active once the MPQ8633A-H starts up. During the LS-FET t_{ON}, I_L is sensed by a current mirror, which generates a current output at the CS pin. The current-sense gain (G_{CS}) ratio is the value of this current output over the actual current.

The current-sense resistor (R_{CS}) connected between the CS and AGND pins makes the current-sense voltage (V_{CS}) proportional to I_L cycle-by-cycle. The HS-FET turns on once V_{CS} drops below the internal over-current protection (OCP) threshold (V_{OCP}) during the LS-FET t_{ON} to limit the inductor valley current cycle-by-cycle.

R_{CS} can be calculated with Equation (3):

$$R_{CS}(\Omega) = \frac{V_{OCP}}{G_{CS} \times (I_{LIMIT} - \frac{(V_{IN} - V_{OUT}) \times V_{OUT}}{V_{IN}} \times \frac{1}{2 \times L \times f_{SW}})} \quad (3)$$

Where V_{OCP} is 1.2V, G_{CS} is 20μA/A, and I_{LIMIT} is the desired current limit in amps (A).

Once the device starts up, hiccup mode is active after a delay time (3ms). If the device detects an over-current (OC) fault for 31 consecutive cycles, or if the V_{FB} drops below the under-voltage protection (UVP) threshold (V_{UVP}), the part enters hiccup mode. In hiccup mode, the HS-FET latches off and the LS-FET latches off during zero-current detection (ZCD). $V_{TRK/REF}$ is also discharged. After about 11ms, the MPQ8633A-H attempts to initiate an SS. If the OC fault is still present after 3ms, then the device repeats this operation until the OC fault is removed, and V_{OUT} ramps up smoothly to its regulation level.

Negative Inductor Current Limit

If the LS-FET detects a negative current (-9A), then the LS-FET turns off for 200ns to limit the negative current.

Output Sink Mode (OSM)

The MPQ8633A-H employs output sink mode (OSM) to regulate V_{OUT} to its targeted value. If V_{FB} exceeds 104% of V_{REF} (and is below V_{OVP}), then the part operates in OSM. In OSM, the LS-FET remains on until the LS-FET current (I_{LS}) reaches the negative I_{LIMIT} (I_{LIMIT_NEG}) (-5.5A). Once I_{LS} reaches -5.5A, the LS-FET turns off for 200ns and the HS-FET turns on. The LS-FET turns on again after 100ns. The MPQ8633A-H continues to operate in OSM until V_{FB} drops below 102% of V_{REF}. Once V_{FB} drops below 102% of V_{REF}, the MPQ8633A-H exits OSM after 15 consecutive cycles of FCCM.

Over-Voltage Protection (OVP)

The MPQ8633A-H monitors V_{OUT} by connecting FB to the tap of the FB resistor divider. The resistor divider detects whether an over-voltage (OV) fault has occurred. This also provides hiccup mode for OVP.

If V_{FB} exceeds 116% of V_{REF}, then OVP is triggered. PGOOD is pulled down until it reaches the low-side I_{LIMIT_NEG}. Once it reaches I_{LIMIT_NEG}, the LS-FET turns off for 200ns, and the HS-FET turns on for the LS-FET t_{OFF}. After 200ns, the LS-FET is turned on again. The MPQ8633A-H continues this operation to try to discharge the excessive voltage on the output. The part exits OVP discharge mode once V_{FB} drops below 105% of V_{REF}.

Thermal Shutdown

The IC monitors the junction temperature (T_J) internally. If T_J exceeds the thermal shutdown threshold (typically 160°C), then the converter shuts down, and the TRK/REF capacitors are discharged. Once T_J drops below 130°C, the IC initiates an SS to resume normal operation. There is about 30ºC hysteresis. Thermal shutdown is a non-latch protection.

Output Voltage Setting and Remote Output Voltage Sensing

Choose a value for R1. Then R2 can be calculated with Equation (4) on page 16:

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$$R2(k\Omega) = \frac{V_{REF}}{V_{OUT} - V_{REF}} \times R1(k\Omega) \quad (4)$$

Connect a feed-forward capacitor (C_{FF}) in parallel with R1 to improve load transient response. R1 and C_{FF} add an extra zero to the system, which improves loop response. R1 and C_{FF} are selected so that the zero formed by R1 and C_{FF} is between 20kHz and 60kHz. The zero (f_{ZERO}) can be calculated with Equation (5):

$$f_{ZERO} = \frac{1}{2\pi \times R1 \times C_{FF}} \quad (5)$$

Power Good (PG)

The PGOOD pin is a power good (PG) output. PGOOD is the open-drain of a MOSFET. Connect PGOOD to VCC or another external voltage source (<3.6V) via a pull-up resistor (e.g. 10kΩ). Once V_{IN} is applied, the MOSFET turns on, and PGOOD is pulled to AGND before TRK/REF is ready. Once V_{FB} exceeds 92.5% of V_{REF}, PGOOD is pulled high after a delay time (0.8ms).

If V_{FB} drops below 80% of V_{REF} or exceeds 116% percent of V_{REF}, then PGOOD is latched low. PGOOD can only be pulled high again after a new SS.

If V_{IN} fails to power the MPQ8633A-H, then PGOOD is clamped low regardless of whether it is tied to an external DC source via a pull-up resistor. Figure 5 shows the relationship between the PGOOD voltage (V_{PG}) and the PGOOD pull-up current (I_{PG}).

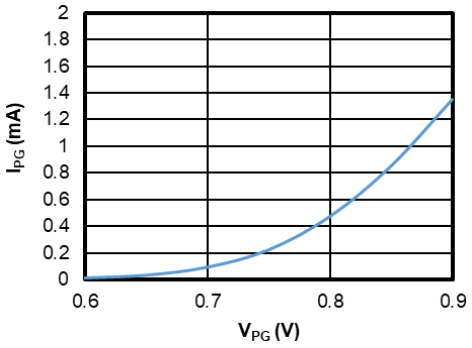


Figure 5: Clamped V_{PG} vs. I_{PG}

Enable (EN) Configuration

The EN pin is an input signal that turns the MPQ8633A-H on and off. Pull EN high to turn the converter on; pull EN low to turn it off. Do not float EN. EN can be driven by an analog or digital control logic signal to enable and disable the device.

The MPQ8633A-H provides accurate EN thresholds. A resistor divider between the VIN and AGND pins can be used to configure the start-up V_{IN} (V_{IN_SU}).

This is highly recommended for applications without a dedicated EN control logic signal to avoid V_{EN} from bouncing between the EN UVLO rising and falling thresholds during start-up and shutdown. V_{IN_SU} can be calculated with Equation (6):

$$V_{IN_SU}(V) = V_{EN_RISING} \times \frac{R_{UP} + R_{DOWN}}{R_{DOWN}} \quad (6)$$

Where V_{EN_RISING} is 1.22V.

Choose R_{UP} and R_{DOWN} so that V_{EN} does not exceed 3.6V once V_{IN} reaches its maximum value.

EN can also be connected to VIN via a pull-up resistor (R_{UP}). Choose R_{UP} so that the maximum EN current (I_{EN_MAX}) is 50μA. R_{UP} can be calculated with Equation (7):

$$R_{UP}(k\Omega) = \frac{V_{IN_MAX}(V)}{0.05(mA)} \quad (7)$$

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APPLICATION INFORMATION

Selecting the **Input Capacitor (C_{IN})**

The step-down converter has a discontinuous input current (I_{IN}), and requires a capacitor to supply AC current to the step-down converter while maintaining the DC V_{IN}. Use ceramic capacitors for the best performance. Place the input capacitors as close to the VIN pin as possible.

The capacitance can vary significantly with the temperature. Capacitors with X5R and X7R dielectrics are recommended due to their stable temperature characteristics and low ESR.

The input capacitors should have a ripple current rating that exceeds the converter's maximum input ripple current (I_{CIN_MAX}). The input ripple current (I_{CIN}) can be estimated with Equation (8):

$$I_{CIN} = I_{OUT} \times \sqrt{\frac{V_{OUT}}{V_{IN}} \times (1 - \frac{V_{OUT}}{V_{IN}})} \quad (8)$$

The worst-case condition occurs at V_{IN} = 2 x V_{OUT}, which can be calculated with Equation (9):

$$I_{CIN} = \frac{I_{OUT}}{2} \quad (9)$$

For simplification, choose an input capacitor (C_{IN}) with an RMS current rating that exceeds half the maximum load current (I_{LOAD_MAX}). C_{IN} determines the converter's V_{IN} ripple (ΔV_{IN}). If there is a ΔV_{IN} requirement in the system, then select C_{IN} to meet the system's specification.

ΔV_{IN} can be calculated with Equation (10):

$$\Delta V_{IN} = \frac{I_{OUT}}{f_{SW} \times C_{IN}} \times \frac{V_{OUT}}{V_{IN}} \times (1 - \frac{V_{OUT}}{V_{IN}}) \quad (10)$$

The worst-case condition occurs at V_{IN} = 2 x V_{OUT}, which can be calculated with Equation (11):

$$\Delta V_{IN} = \frac{1}{4} \times \frac{I_{OUT}}{f_{SW} \times C_{IN}} \quad (11)$$

Selecting the Output Capacitor (C_{OUT})

The output capacitor (C_{OUT}) maintains the DC V_{OUT}. Use POSCAP or ceramic capacitors for the best performance. The V_{OUT} ripple (ΔV_{OUT}) can be estimated with Equation (12):

$$\Delta V_{OUT} = \frac{V_{OUT}}{f_{SW} \times L} \times (1 - \frac{V_{OUT}}{V_{IN}}) \times (R_{ESR} + \frac{1}{8 \times f_{SW} \times C_{OUT}}) \quad (12)$$

When using ceramic capacitors, the capacitance dominates the impedance at f_{SW}. The capacitance also dominates ΔV_{OUT}. For simplification, ΔV_{OUT} can be estimated with Equation (13):

$$\Delta V_{OUT} = \frac{V_{OUT}}{8 \times f_{SW}^{\ 2} \times L \times C_{OUT}} \times (1 - \frac{V_{OUT}}{V_{IN}}) \quad (13)$$

When using POSCAP capacitors, the ESR dominates the impedance at f_{SW}. For simplification, ΔV_{OUT} can be estimated with Equation (14):

$$\Delta V_{OUT} = \frac{V_{OUT}}{f_{SW} \times L} \times (1 - \frac{V_{OUT}}{V_{IN}}) \times R_{ESR} \quad (14)$$

Selecting the Inductor

The inductor supplies a constant current to the output load while being driven by the switching V_{IN}. A larger-value inductor results in less ripple current and a lower ΔV_{OUT}; however, a larger-value inductor has a larger physical size, a higher series resistance, and a lower saturation current. Choose an inductor so that the peak-to-peak inductor ripple current (ΔI_L) is between 30% and 40% of the maximum output DC load current. The peak inductor current (I_{L_PEAK}) should be below the maximum output DC load current. The inductance (L) can be calculated with Equation (15):

$$L = \frac{V_{OUT}}{f_{SW} \times \Delta I_L} \times (1 - \frac{V_{OUT}}{V_{IN}}) \quad (15)$$

Choose an inductor that will not saturate under the maximum I_{L_PEAK}. I_{L_PEAK} can be calculated with Equation (16):

$$I_{L_PEAK} = I_{OUT} + \frac{V_{OUT}}{2 \times f_{SW} \times L} \times (1 - \frac{V_{OUT}}{V_{IN}}) \quad (16)$$

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PCB Layout Guidelines

Efficient PCB layout is critical for stable operation. For the best performance, refer to Figure 6 and follow the guidelines below:

1. Place the input MLCC capacitors as close to the VIN and PGND pins as possible.
2. Place the major MLCC capacitors on the same layer as the IC.
3. Maximize the VIN and PGND copper plane to minimize the parasitic impedance.
4. Connect a ≥1µF capacitor (0402) to VIN on the right side of the IC. VIN is extended to the right to connect this capacitor.
5. Place two or more 20mil/10mil vias on the inner solid ground plane. Place these via on the ground side of the capacitor.
6. Place multiple vias as close to PGND as possible to minimize both parasitic impedance and thermal resistance.
7. Place the VCC decoupling capacitor close to the IC.
8. Connect the AGND and PGND pins at the point of the VCC capacitor's ground connection.
9. Place a 0.1µF to 1µF BST capacitor as close to the BST and SW pins as possible.
10. Route the BST path using ≥20mil trace width.
11. Place the TRK/REF capacitor close to the TRK/REF and RGND pins.
12. If a via must be placed on the PGOOD pad, place it at least 10mm away from the positive side of the first input decoupling capacitor. Place this via close to the IC.

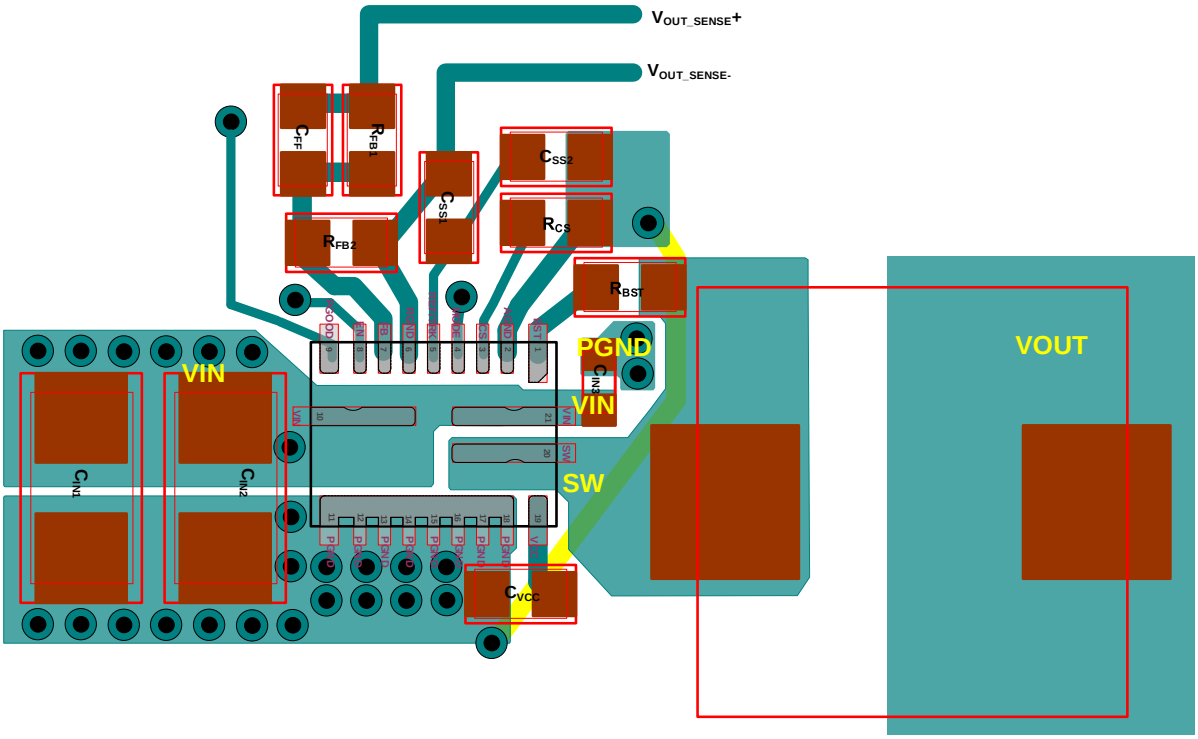
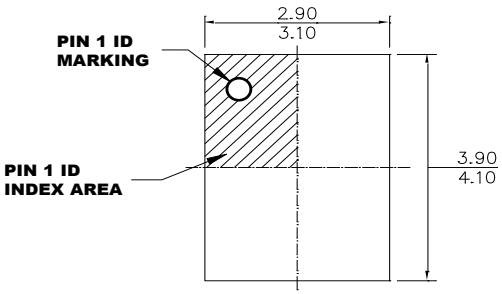


Figure 6: Recommended PCB Layout

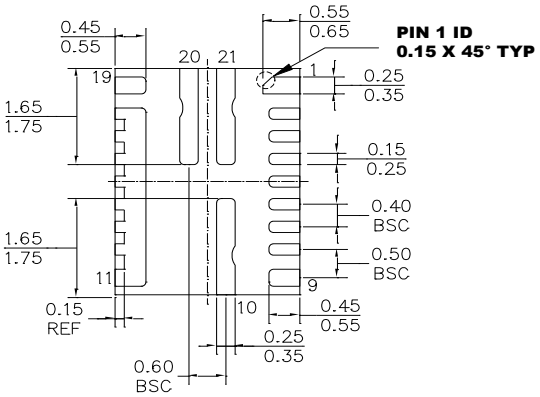
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PACKAGE INFORMATION

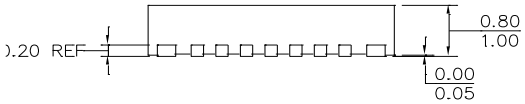
QFN-21 (3mmx4mm)



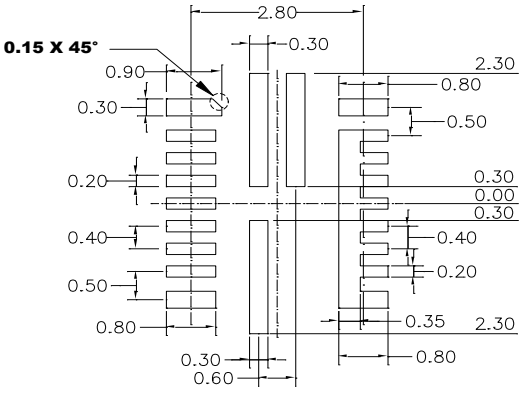
TOP VIEW



BOTTOM VIEW



SIDE VIEW



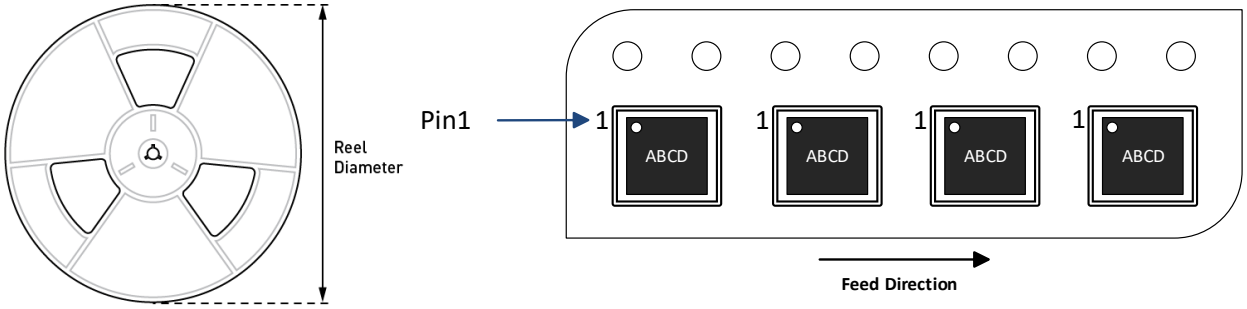
RECOMMENDED LAND PATTERN

NOTE:

1) LAND PATTERN OF PIN1,9,10,11,19,20 AND 21 HAVE THE SAME WIDTH.
2) ALL DIMENSIONS ARE IN MILLIMETERS.
3) LEAD COPLANARITY SHALL BE 0.08 MILLIMETERS MAX.
4) JEDEC REFERENCE IS MO-220.
5) DRAWING IS NOT TO SCALE.

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CARRIER INFORMATION



Part Number	Package Description	Quantity/ Reel	Quantity/ Tube	Reel Diameter	Carrier Tape Width	Carrier Tape Pitch
MPQ8633A-HGLE-Z	QFN-21 (4mmx3mm)	5000	N/A	13in	12mm	8mm

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REVISION HISTORY

Revision #	Revision Date	Description	Pages Updated
1.0	4/19/2022	Initial Release	-

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